

APPENDIX I
COIL DESIGN

The theory of coil design is based on the work of Campbell¹ (1959) and others. Time varying magnetic flux, Φ_m , cutting a coil will induce an e.m.f. across the coil terminals which according to Faraday's Law of induction is

$$\text{e.m.f.} = - \frac{d\Phi_m}{dt}$$

In our case there are N turns, or N circuits in series so that the voltage across the coil terminals is

$$V = -N \frac{d\Phi_m}{dt}$$

Since

$$\Phi_m = \int \vec{B} \cdot d\vec{s}$$

the voltage output from a circular coil with area A is

$$V = -NA \frac{dB}{dt}$$

Assuming B to oscillate sinusoidally at frequency ω

$$V = NA\omega B \quad (1)$$

This equation is generally true for induction coils so long as ω is well below the resonant frequency of the coil in a frequency range where the coil acts as a purely resistance circuit element.

In practical units, the voltage can be expressed as

$$V = NA 10^{-7} 2\pi f B \quad (2)$$

¹ Campbell, op. cit., p. 7.

Where V is in μV , A is in cm^2 , and β is in γ [$\gamma = 10^{-5}$]

The coils that we built each had 20,100 turns on a two-meter diameter circular frame so that the NA product is $6.315 \times 10^8 \text{ turn-cm}^2$ the Eq.2 becomes

$$V = 396.8 \text{ fB } \mu\text{V} \quad (3)$$

We designed the coils to be sensitive in the Frequency range of Pc 1 and they can detect the signals from 0.001 to 10 Hz.

The resonant frequency of the coil is approximately

$$\omega_0 = \left(\frac{1}{LC} \right)^{\frac{1}{2}}$$



To fix ω_0 well above the frequencies of interest, the coil inductance or capacitance must be kept reasonably small. Decreasing of value of L can only be done by reducing the number of turns (L varies as N^2) but this has the unfavorable result of loss of sensitivity at the frequencies of interest. On the other hand, C can be decreased, with no loss of sensitivity, by careful winding. One practice is to keep small the number of turns in a winding layer so that the number of layers will increase but the layer-to-layer capacitance between adjacent layer will decrease. The total capacitance also decreased because, in the coil, it looks like capacitors connected in series; so,

$$C = \frac{C_1}{M}$$

where C = total capacitance of the coil

C_1 = the individual layer-to-layer capacitance

M = the number of layer

Hence when M is larger the total capacitance will be a small value.

APPENDIX II
COIL CALIBRATION

The calibration technique used to determine the inductance, capacitance, and resonant frequency consists of first measuring the coil resistance (R_c) on a bridge, and then applying a voltage V , over a wide range of frequencies alternately to the coil and to a dummy resistor R_D , $R_D = R_c$. The voltage drop V_2 across a resistor R_g in series with the source is recorded at each frequency and a plot of the ratio

$$n = \frac{V_2(\text{coil})}{V_2(\text{dummy})} \quad (1)$$

From this curve we can estimate values of L and C , as described below. The measuring circuit used is shown in Figure 21.

The ratio n can be shown equal to the ratio of two impedances. At any frequency, ω ,

$$n(\omega) = \frac{R_g + Z(\omega)}{R_g + R_D}$$

where Z is the coil impedance, and R_g is selected to be much larger than R_c ,

$$|Z| = \frac{L}{R_c C} \left[\frac{1 + \frac{R_c^2}{\omega^2 L^2}}{1 + \left(\frac{\omega L - 1/\omega C}{R_c} \right)^2} \right]^{\frac{1}{2}}$$

At frequencies approaching DC, $Z \rightarrow R_c$ and

$$\lim_{\omega \rightarrow 0} n = \frac{1 + \frac{R_c}{R_g}}{1 + \frac{R_D}{R_g}} \rightarrow \frac{1 + \frac{R_c}{R_g}}{1 + \frac{R_D}{R_g}} \rightarrow 1$$



On the other hand, at very high frequencies coil inductive reactance also becomes very large so that

$$Z \rightarrow -i \left(\frac{1}{\omega C} \right)$$

and

$$\omega \rightarrow \infty \quad n = \frac{\left| R_g - i \left(\frac{1}{\omega C} \right) \right|}{R_g + R_D} = \frac{\left(1 + \frac{1}{R^2 \omega^2 C^2} \right)^{1/2}}{1 + \frac{R_D}{R_g}}$$

So long as R_g is very large

$$\omega \rightarrow \infty \quad n \rightarrow 1$$

Between these extremes there will exist a frequency, the resonant frequency, where $|R_g + Z|$, and thus n , is a maximum. It can be shown that Z takes on its largest value,

$$Z = \frac{L}{R_c C}$$

of

$$\omega_o = \left[\frac{1}{LC} - \left(\frac{R_c}{L} \right)^2 \right]^{1/2} \quad (2)$$

where

$$n = n_{\max} = 1 + \frac{L}{R_c R_g C} \quad (3)$$

We find through simple algebraic manipulation that

$$L = (n_{\max} - 1) R_c R_g C$$

As ω_0 can be determined by finding the ω at which n is a maximum, the coil C may now be found using values of ω_0 , R_c , and L in Eqs. (2) and (3).

$$C = \frac{\left[\frac{(n_{\max} - 1) R_g}{R_c} - 1 \right]^{\frac{1}{2}}}{\omega_0 (n_{\max} - 1) R_g}$$

As Campbell points out, in actual measurement there exists an effective series resistance of the voltage source and a shunt capacitance of the measuring device. These two circuit parameters tend to cause n to become less than unity at high frequencies, but they do not change the L and C estimates.

APPENDIX III

CHOICE OF SAMPLING INTERVAL AND OTHER PARAMETER

The data to be analyzed is recorded continuously and must be digitized prior to machine analysis.

Sampling Interval: The sampling interval $h = \Delta t$ is usually chosen such that

$$h = \frac{1}{2f_{\max}}$$

Since $\frac{1}{f_{\max}}$ is the smallest period that can be observed in the record, h must be chosen sufficiently small so that aliasing¹ will not be a problem.

By definition there will be only 2 points per cycle of the f_{\max} oscillation, but if signal frequencies of large amplitude exist near f_{\max} , one should choose $h = \frac{1}{4f_{\max}}$. If power spectra measurements are the prime consideration, then choosing $h = \frac{2}{5f_{\max}}$ is sufficient, but for reasons of computation economy $h = \frac{1}{2f_{\max}}$ can be chosen.

Number of Correlation Lag Values: The maximum number of correlation lag values, m , to be computed depends on the resolution bandwidth, B_e , desired in the power spectra, as well as the sampling interval, h , chosen;

$$m = \frac{1}{B_e h}$$

thus B_e will be small for a given h when m is large.

Sample Size N and Record Length T_r : In choosing sample size N we must consider the standard error of the spectral calculation. In this case N is expressed as

¹ Bendat and Piersol, op. cit., p. 23.

$$N = \frac{m}{\epsilon^2}$$

ϵ is the normalized standard error desired for spectral calculations. As the associated record length, T_r , is

$$T_r = Nh$$

we can easily express the error of autocorrelation or power spectrum estimate in terms of m and N ,

$$\epsilon = \sqrt{\frac{m}{N}}$$

Thus, ϵ will be small for a given N when m is small. In practice it is desirable to keep the maximum lag,

$$m < 0.1N$$

APPENDIX IV
HANNING METHOD



The Hanning method is one way of smoothing periodograms (raw estimates). The power spectral density, $\tilde{G}_x(f)$, is given by equation:

$$\tilde{G}_x(f) = 4 \int_0^m R_x(\tau) \cos(2\pi f\tau) d\tau$$

However, this is an inefficient estimate of the true spectral density and smoothing is necessary.

Let $\tilde{G}_k = \tilde{G}_x(f) = \tilde{G}_x\left(\frac{kf_{\max}}{m}\right)$

when the index k is called the harmonic number, and \tilde{G}_k is the "raw" estimate of the power spectral density function at harmonic k , corresponding to the frequency $f = \frac{kf_{\max}}{m}$.

Let \hat{G}_k represent the "smooth" estimate at harmonic k , where the \wedge replaces the \sim . Then at the $m+1$ frequencies $f = \frac{kf_{\max}}{m}$; $k = 0, 1, 2, 3, \dots, m$ one obtains

$$\hat{G}_0 = 0.5 \tilde{G}_0 + 0.5 \tilde{G}_1$$

$$\hat{G}_k = 0.25 \tilde{G}_{k-1} + 0.5 \tilde{G}_k + 0.25 \tilde{G}_{k+1} \quad k = 1, 2, 3, \dots, m-1.$$

and $\hat{G}_m = 0.5 \tilde{G}_{m-1} + 0.5 \tilde{G}_m$

The upper equation is implemented easily on a binary digital computer compared to other smoothing procedures. These other procedures provide different bias uncertainly errors which may be preferred for certain applications. In general, the Hanning method should be satisfactory for our uses.



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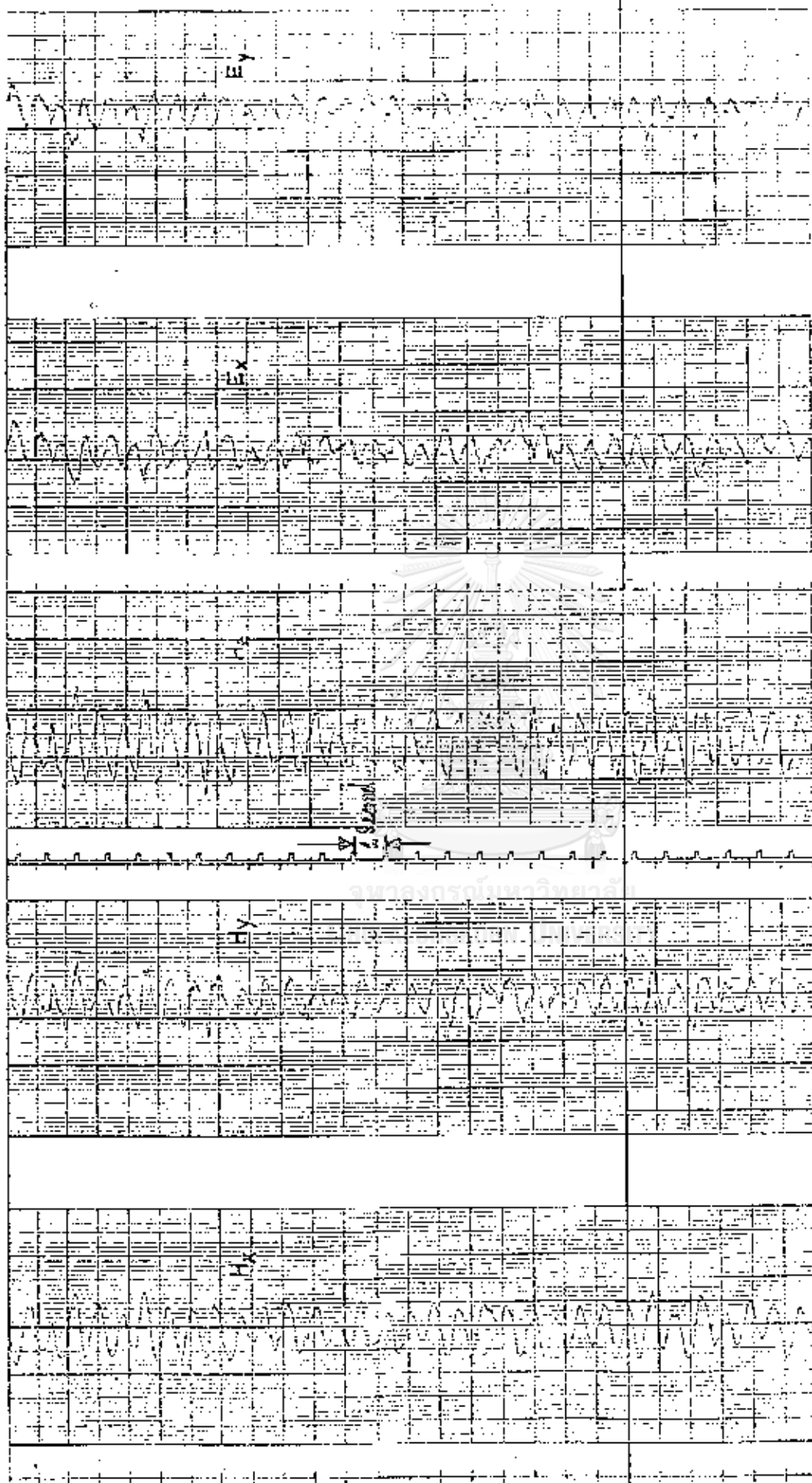
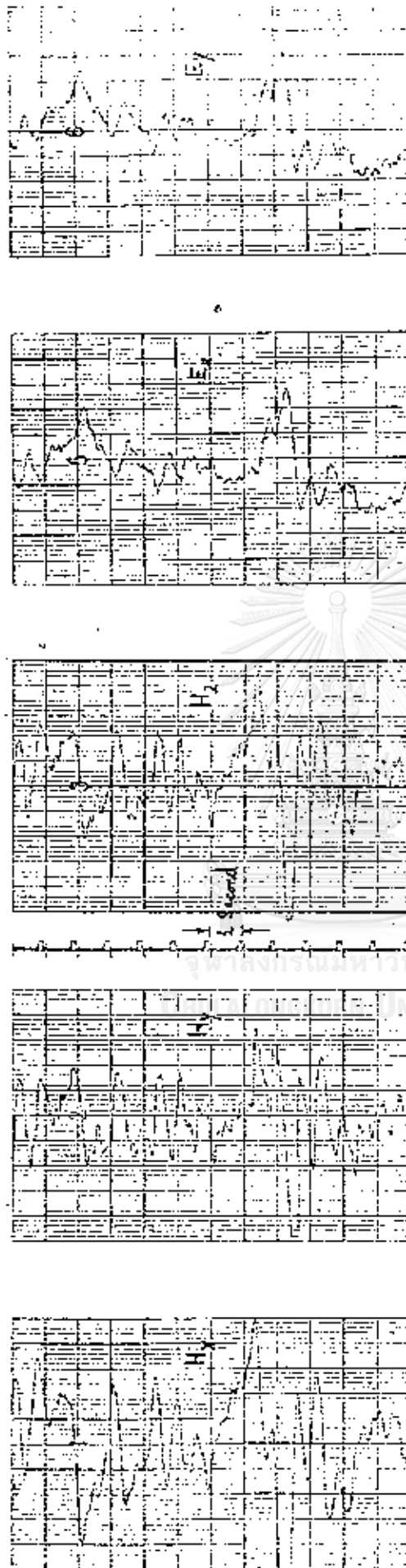


FIG. 1 EXAMPLE OF P_c TYPE MICROPULSATION

FIG. 2 EXAMPLE OF P_i TYPE MICROPULSATION

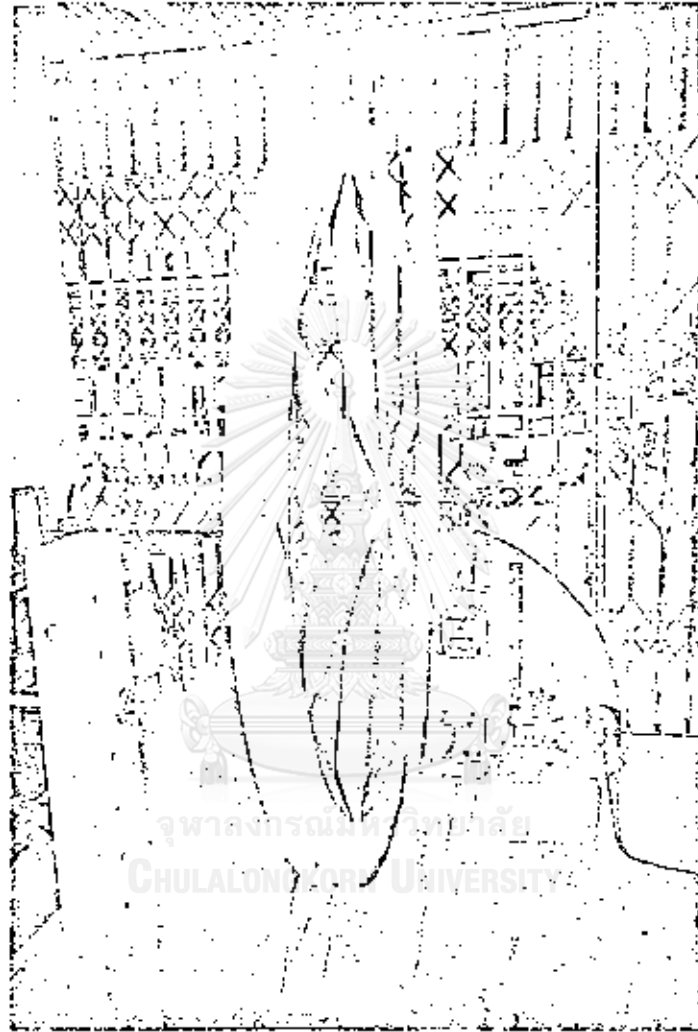
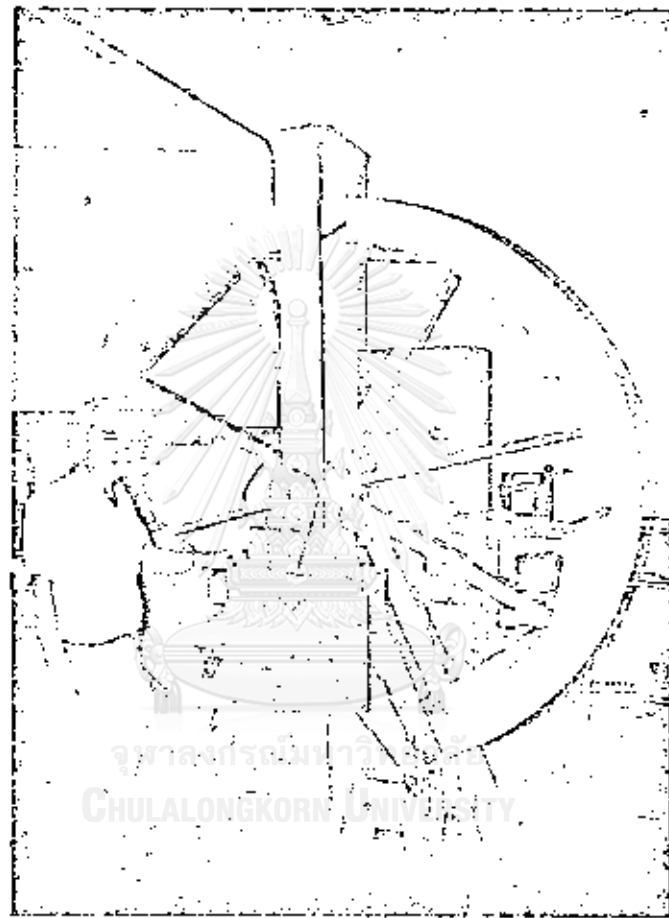


FIG. 3 CLOSE-UP VIEW OF ELECTRIC MOTOR, PULLEY ARRANGEMENT AND TURNS COUNTER



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FIG. 4 COIL FRAME MOUNTED IN WINDING FRAME

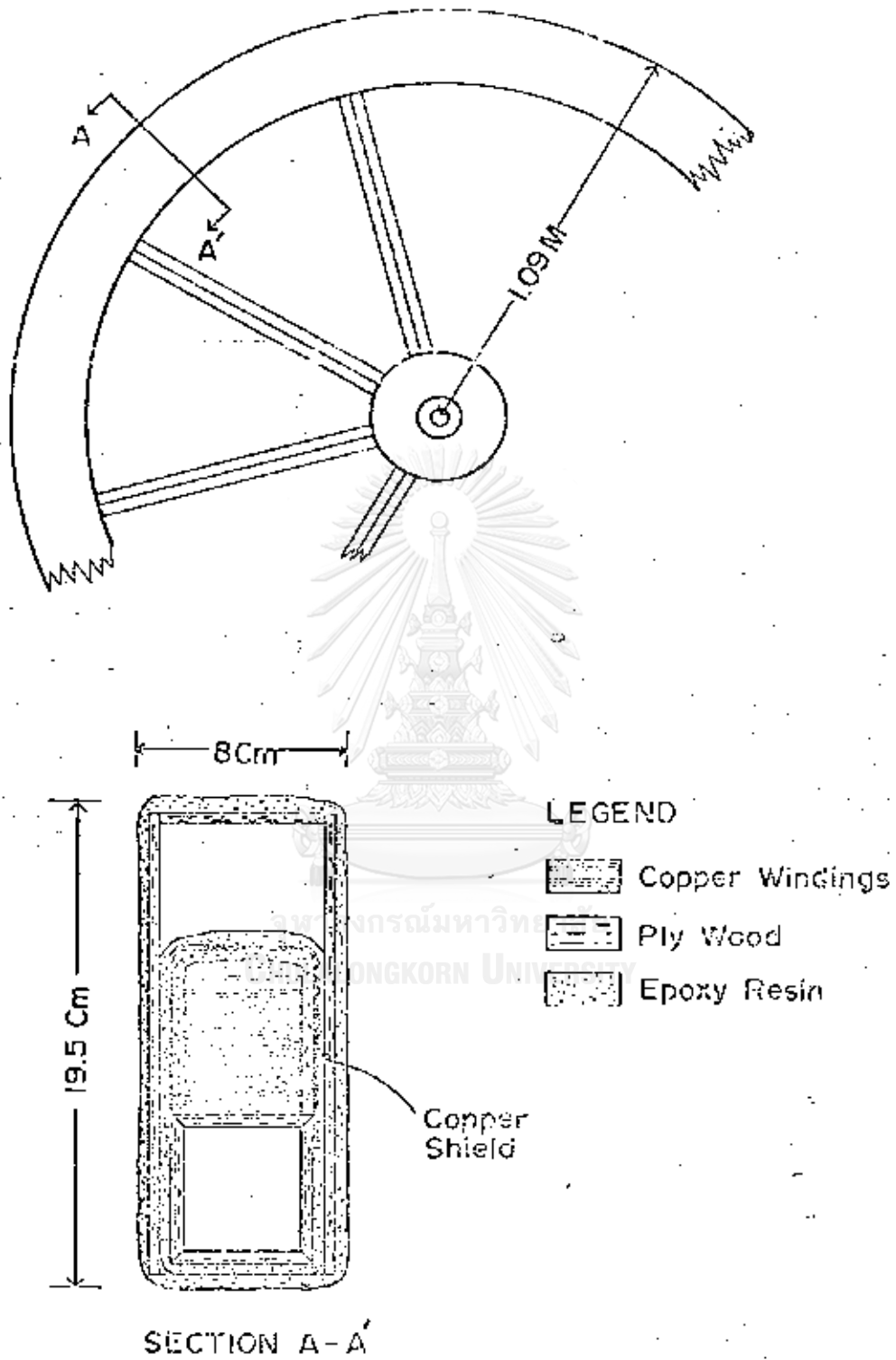


FIG. 5 COIL SCHEMATIC

TYPE 40
SEMI-LOGARITHMIC
5 CYCLES X 10 DIVISIONS
40 3490
MADE IN U.S.A.
KUFFEL & CO. CO.

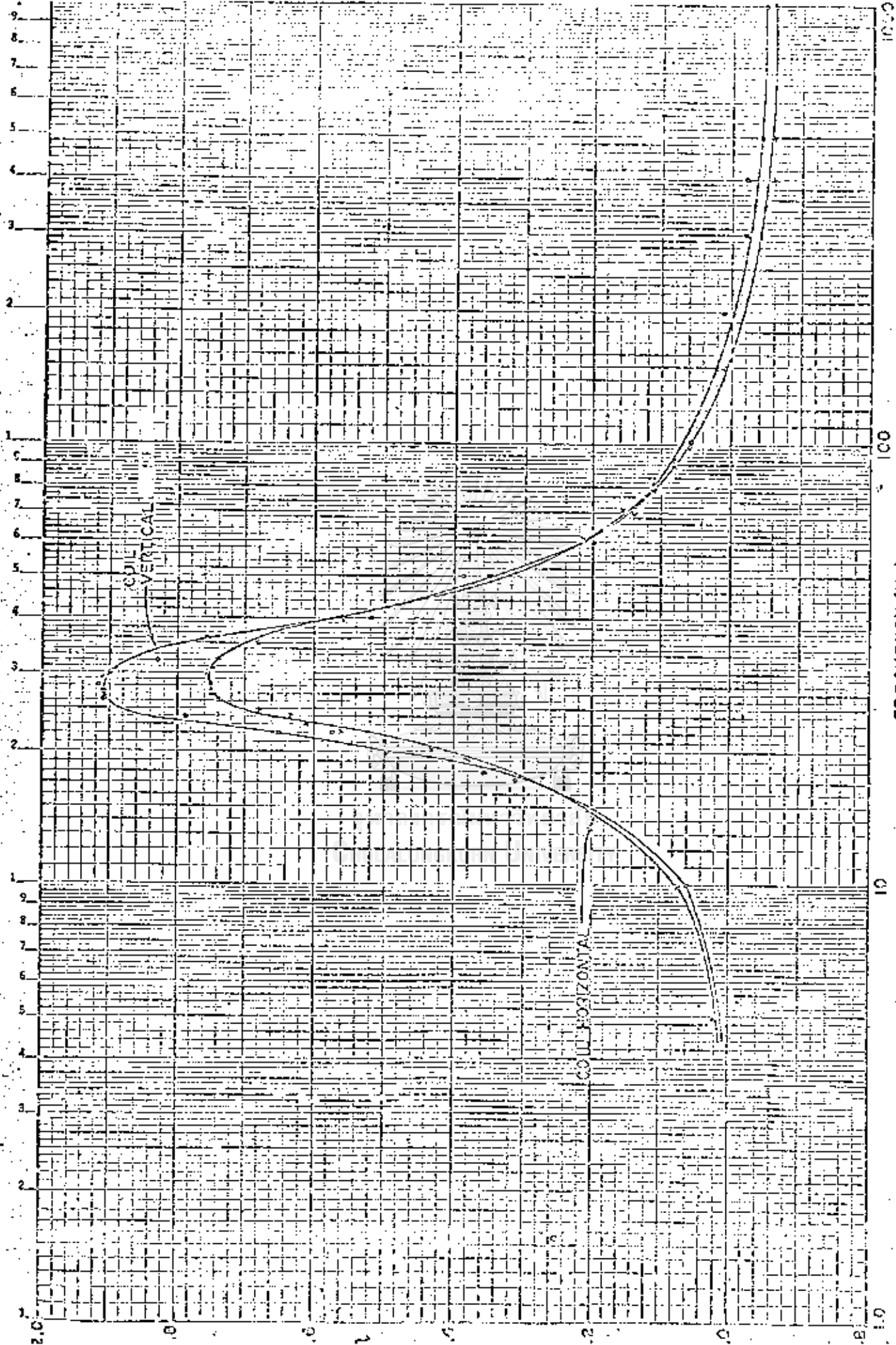


FIG. 6 CALIBRATION CURVE, COIL 2

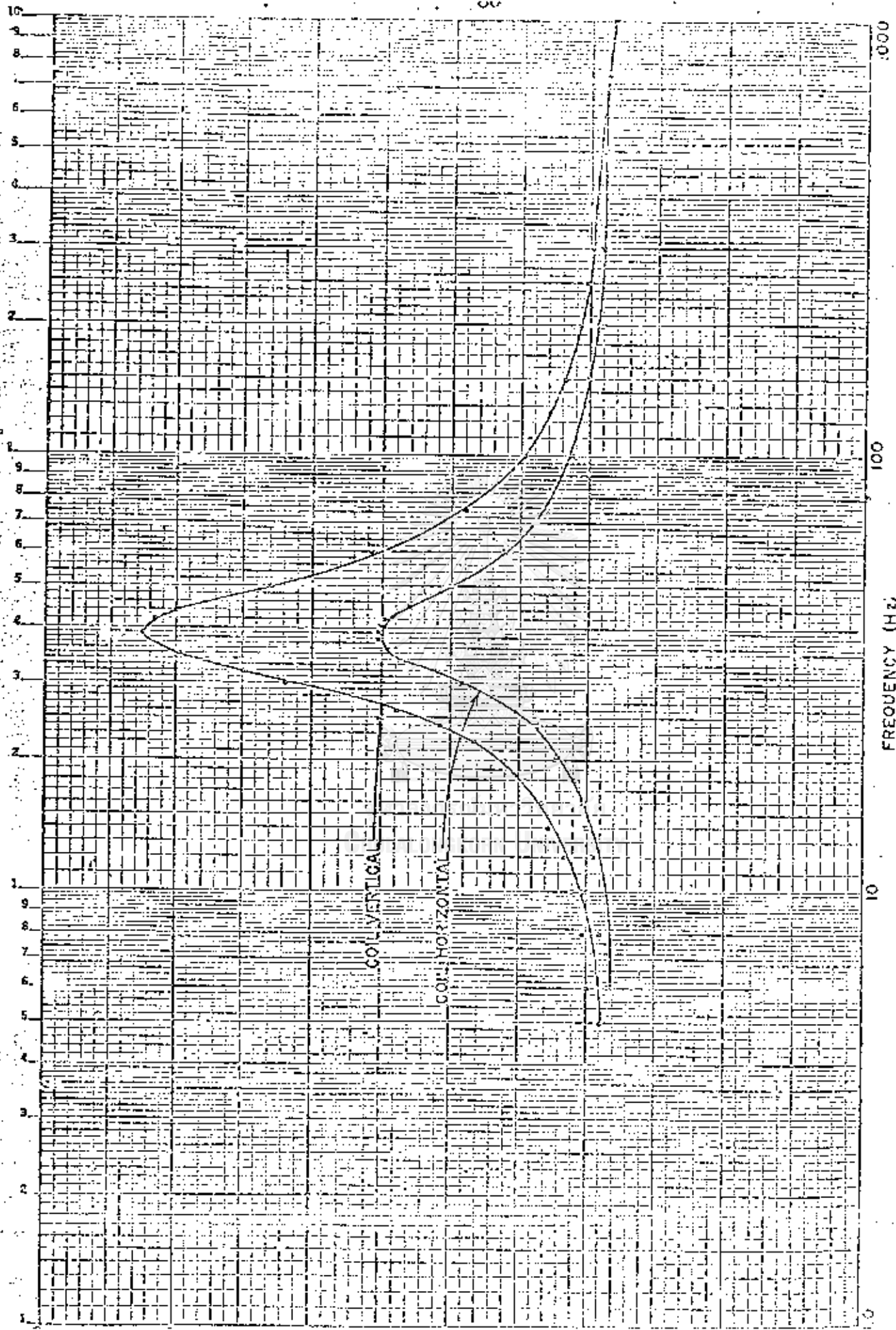


FIG. 7 CALIBRATION CURVE, COIL 3

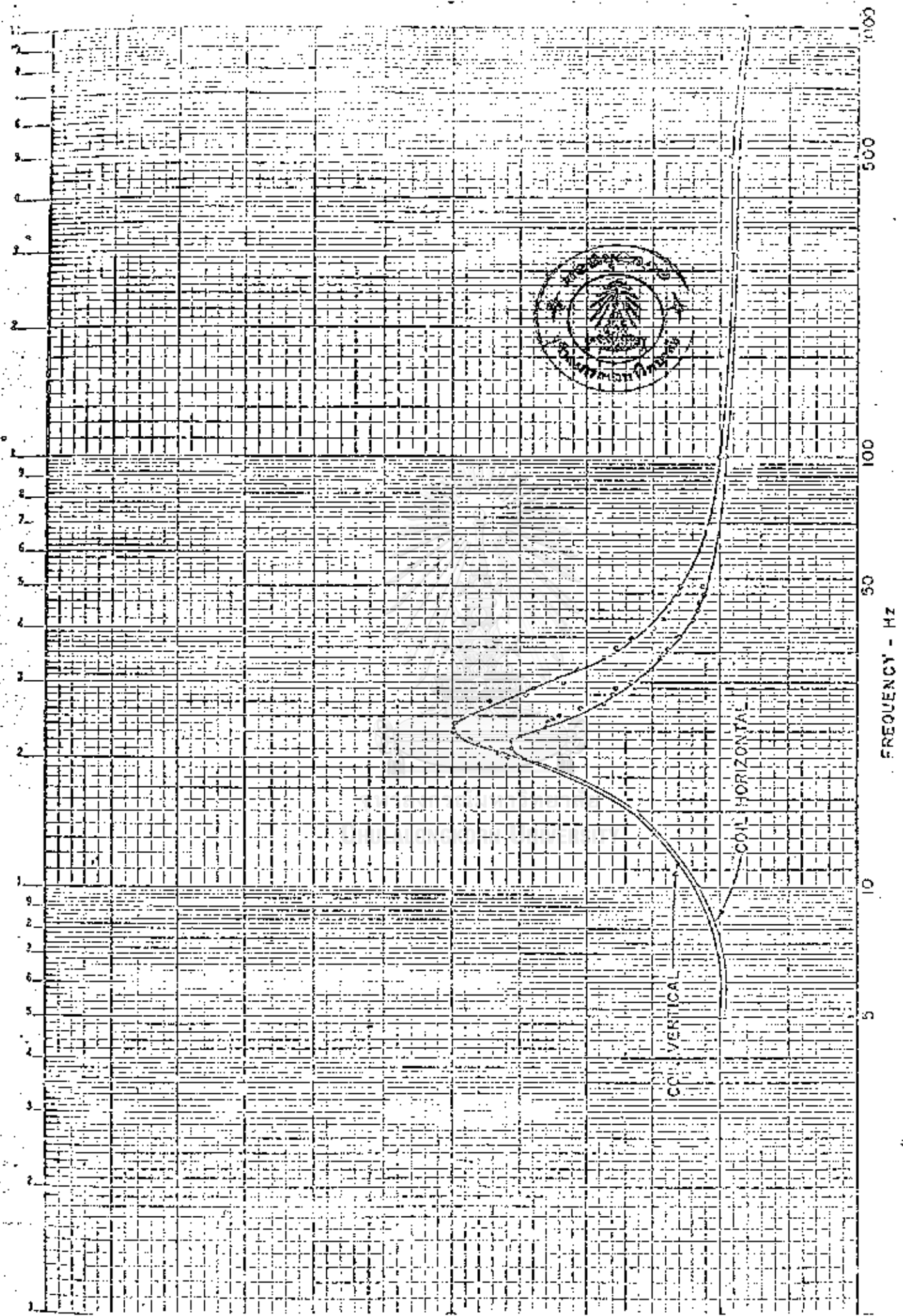


FIG. 8 CALIBRATION CURVE, COIL 4

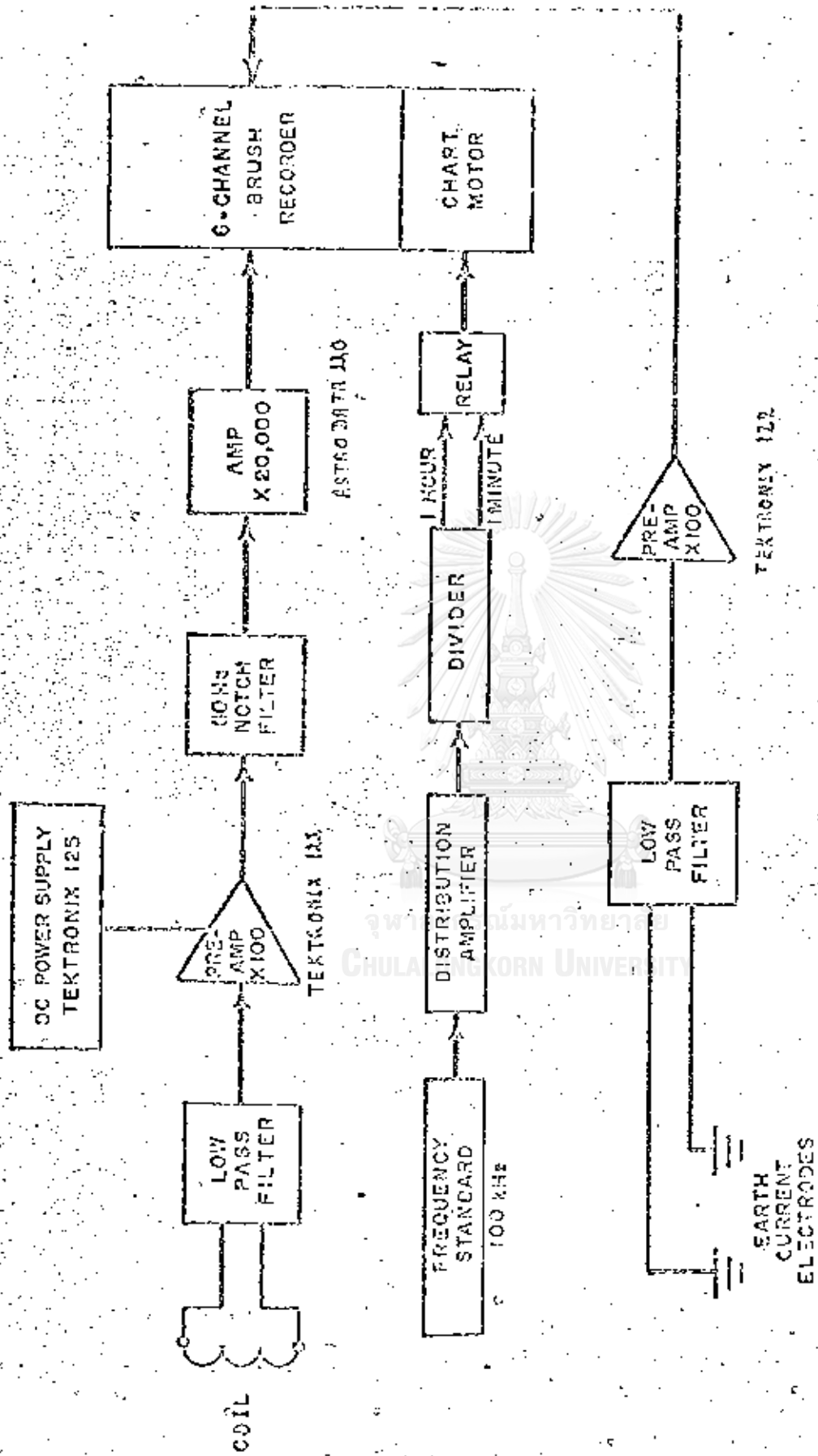


FIG. 9a. BLOCK DIAGRAM OF MAGNETIC AND ELECTRIC FIELD MEASURING SYSTEM

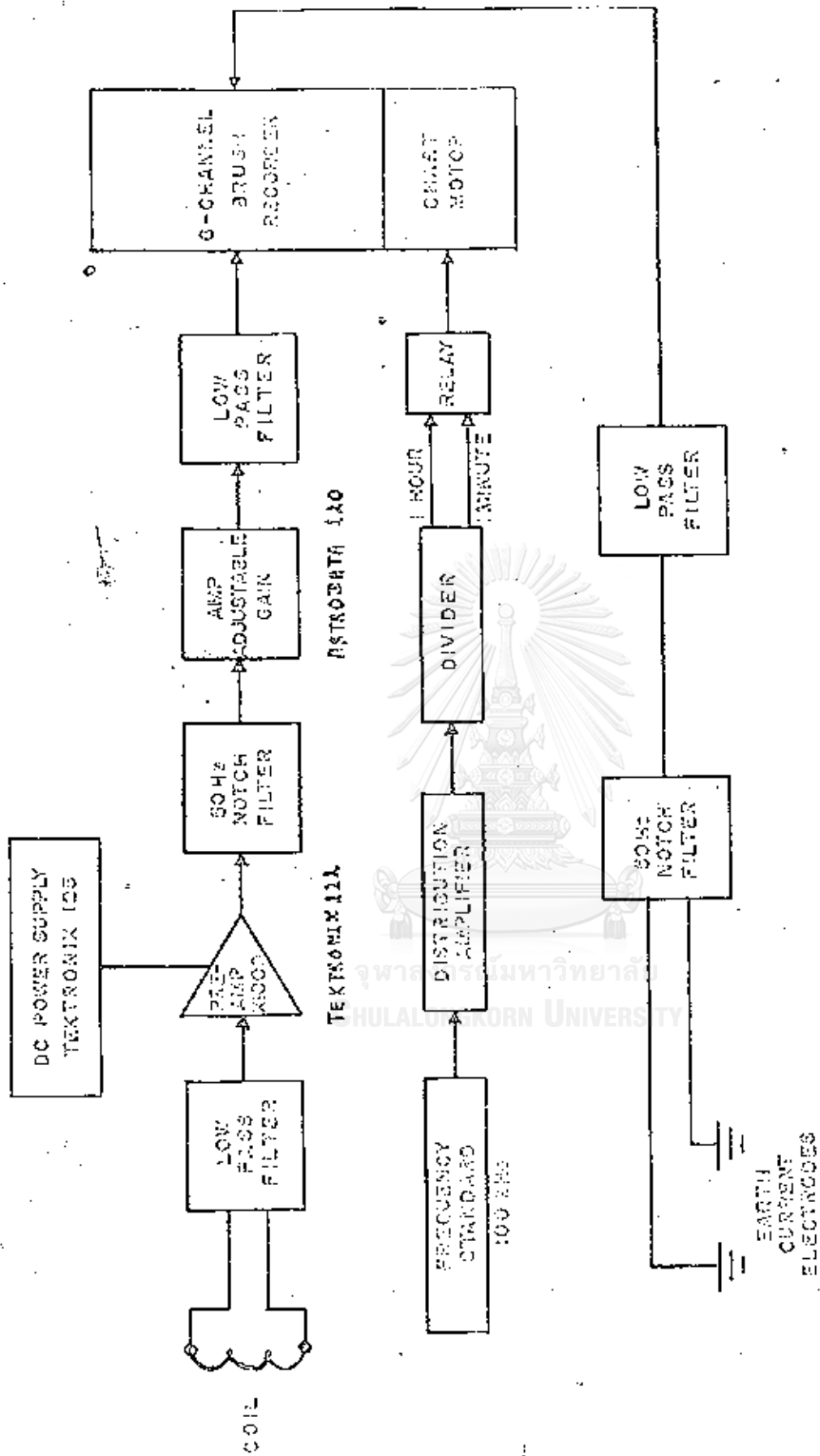


FIG. 9b. BLOCK DIAGRAM OF MAGNETIC AND ELECTRIC FIELD MEASURING SYSTEM

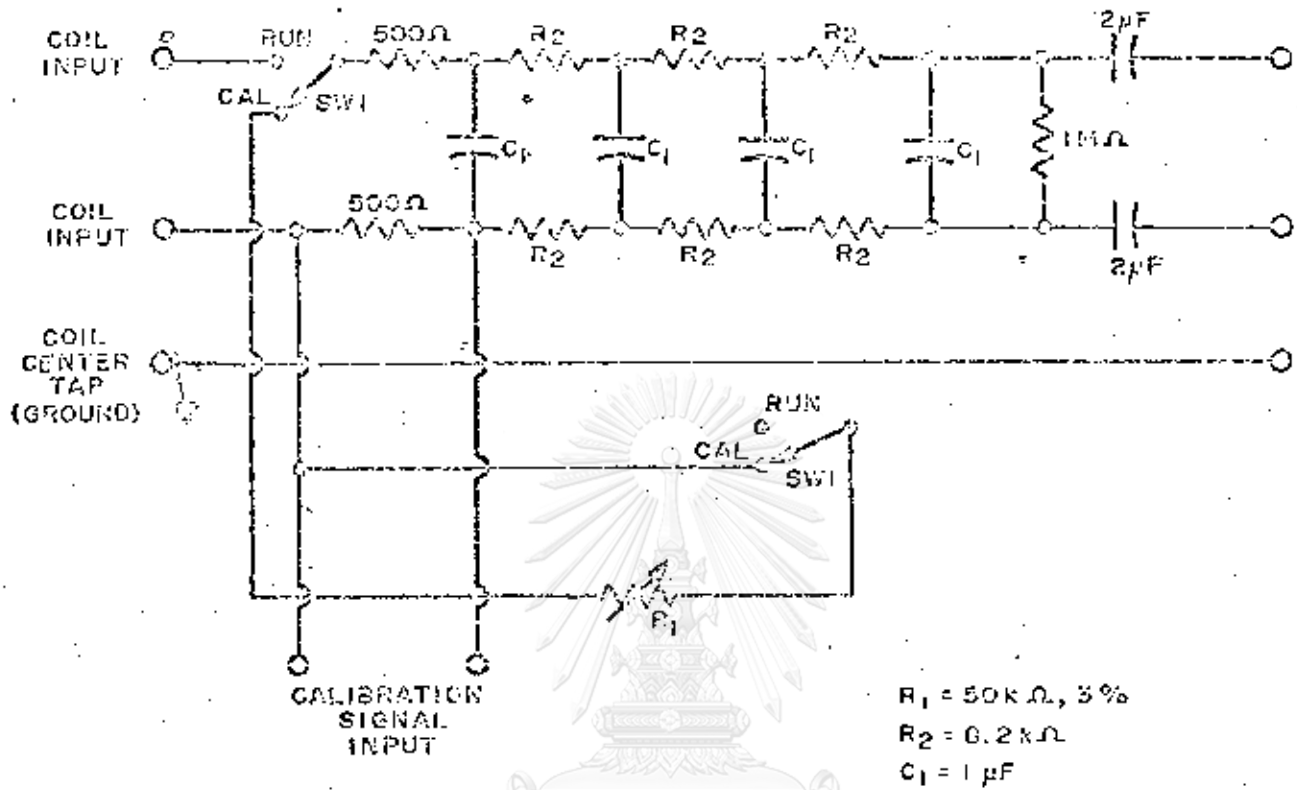


FIG. 10 INITIAL LOW PASS FILTER AND CALIBRATION CIRCUIT FOR COIL MAGNETOMETERS

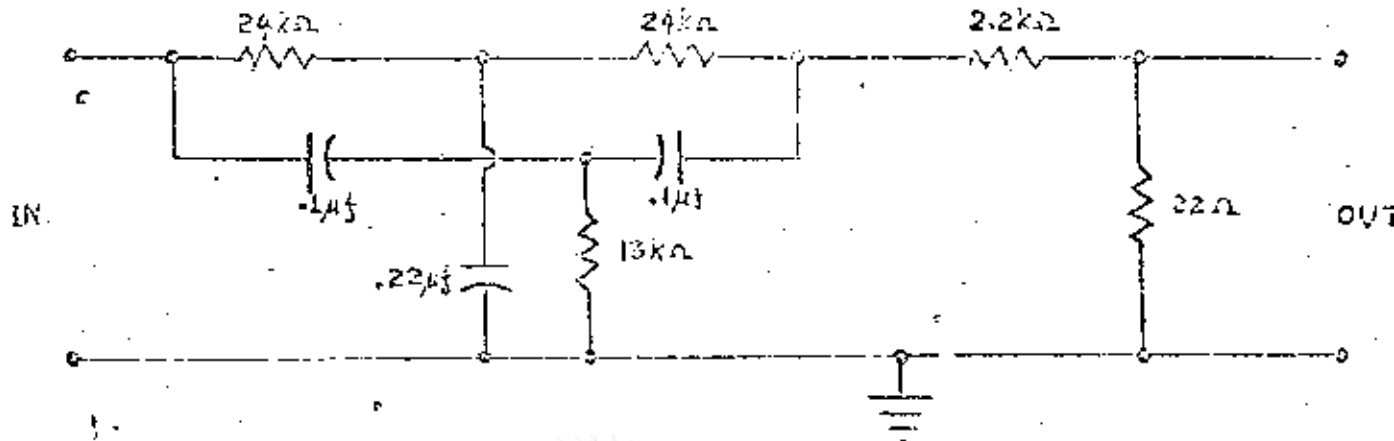


FIG. 11a. 60 Hz NOTCH FILTER AND ATTENUATOR

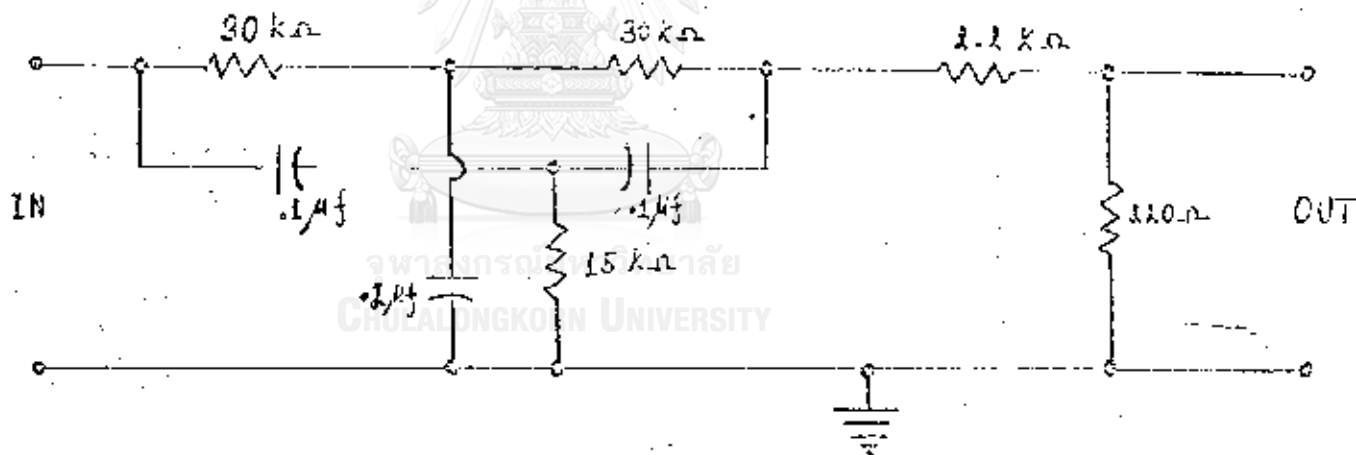


FIG. 11b. 50 Hz NOTCH FILTER AND ATTENUATOR



FIG. 12 PRE-RECORDING LOW-PASS FILTER

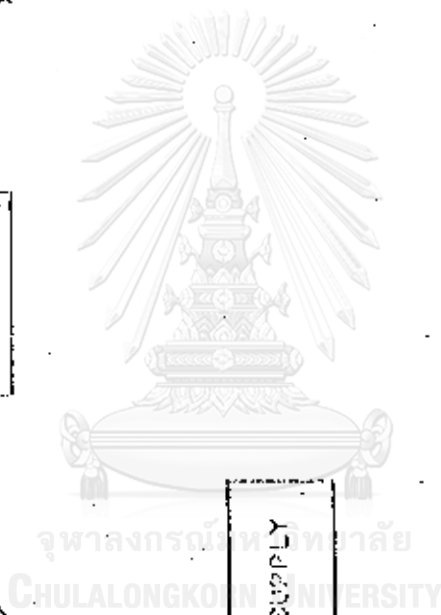
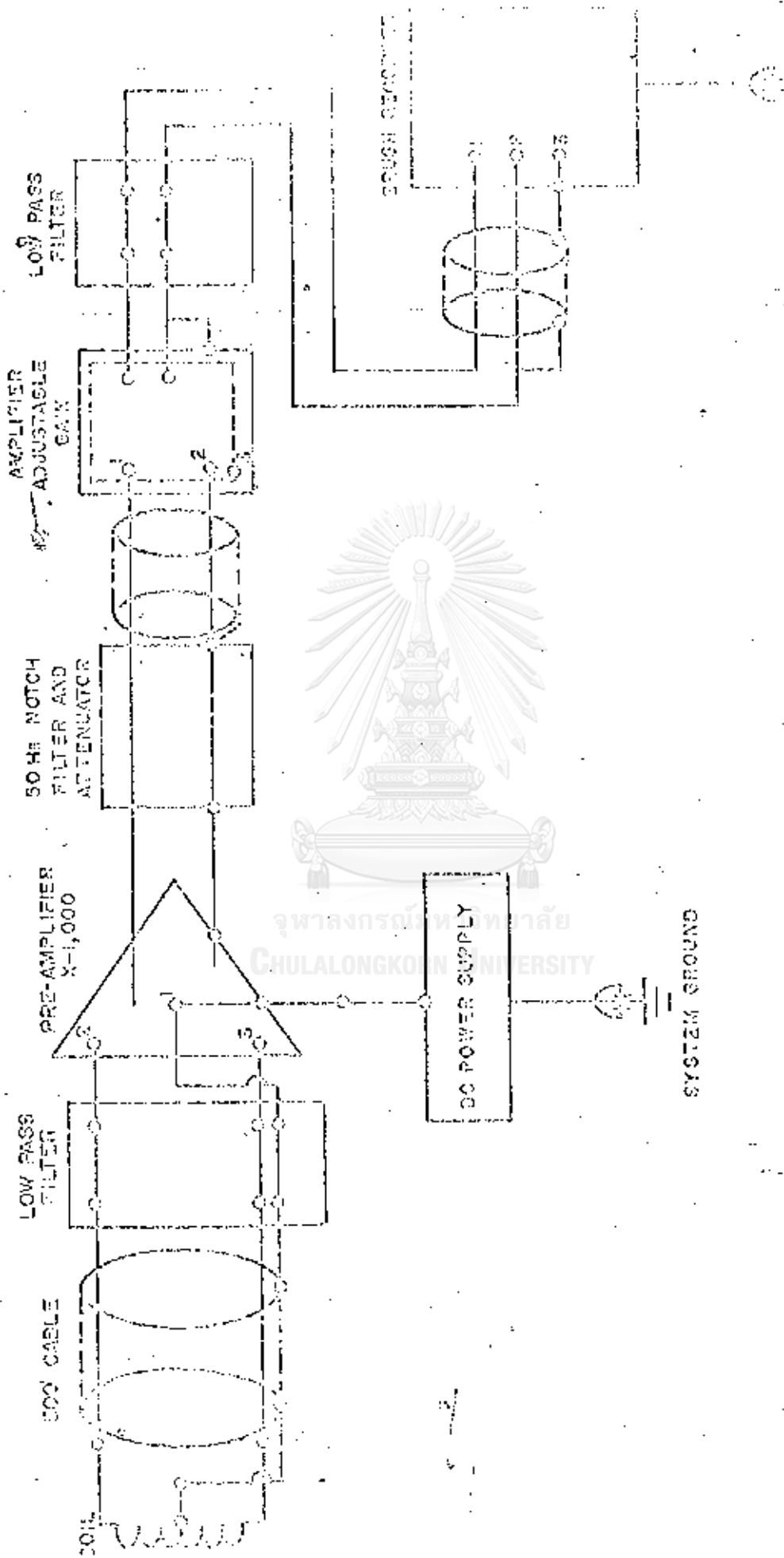


FIG. 13 BLOCK DIAGRAM OF INDUCTION COIL MAGNETOMETER CIRCUIT

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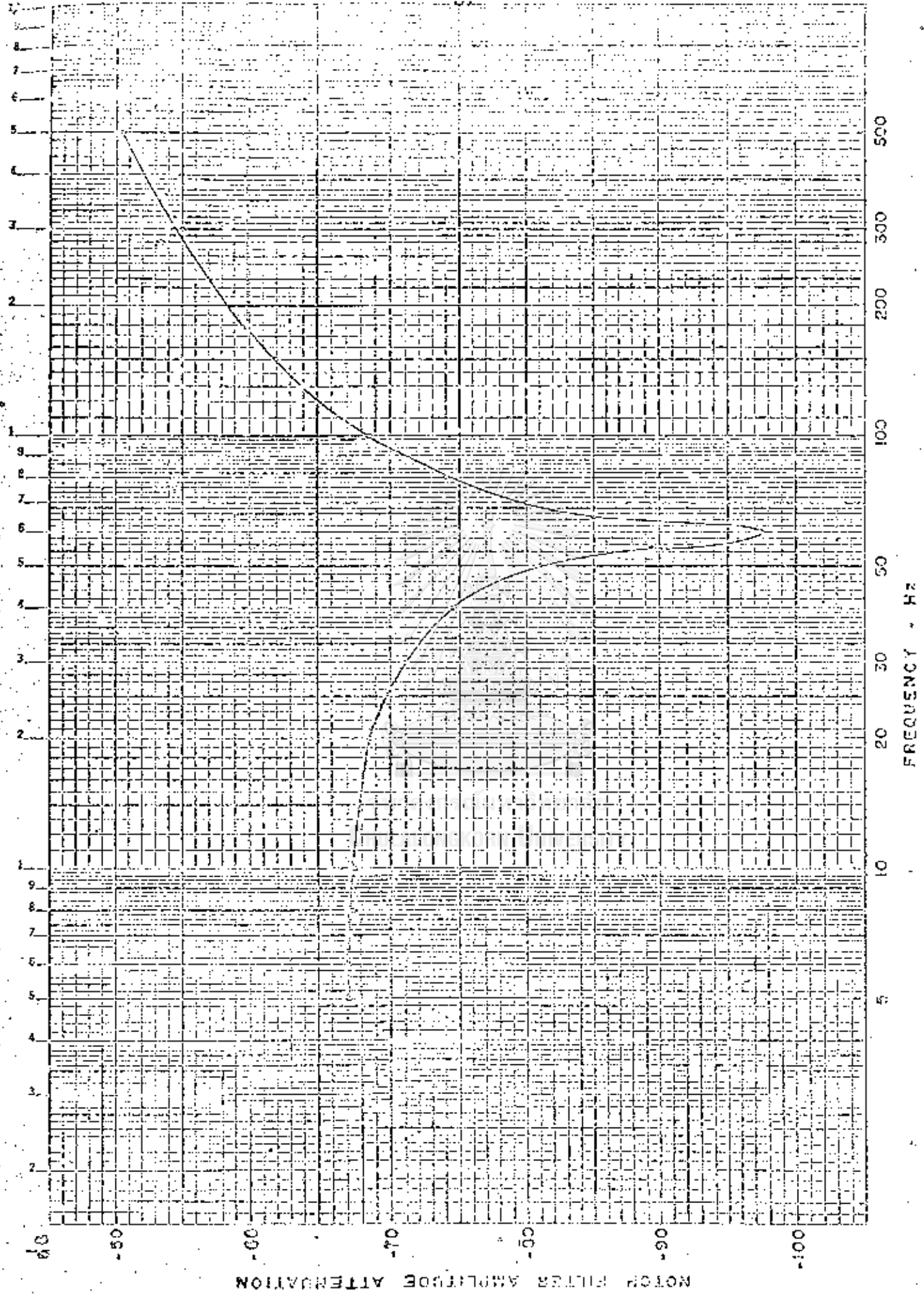
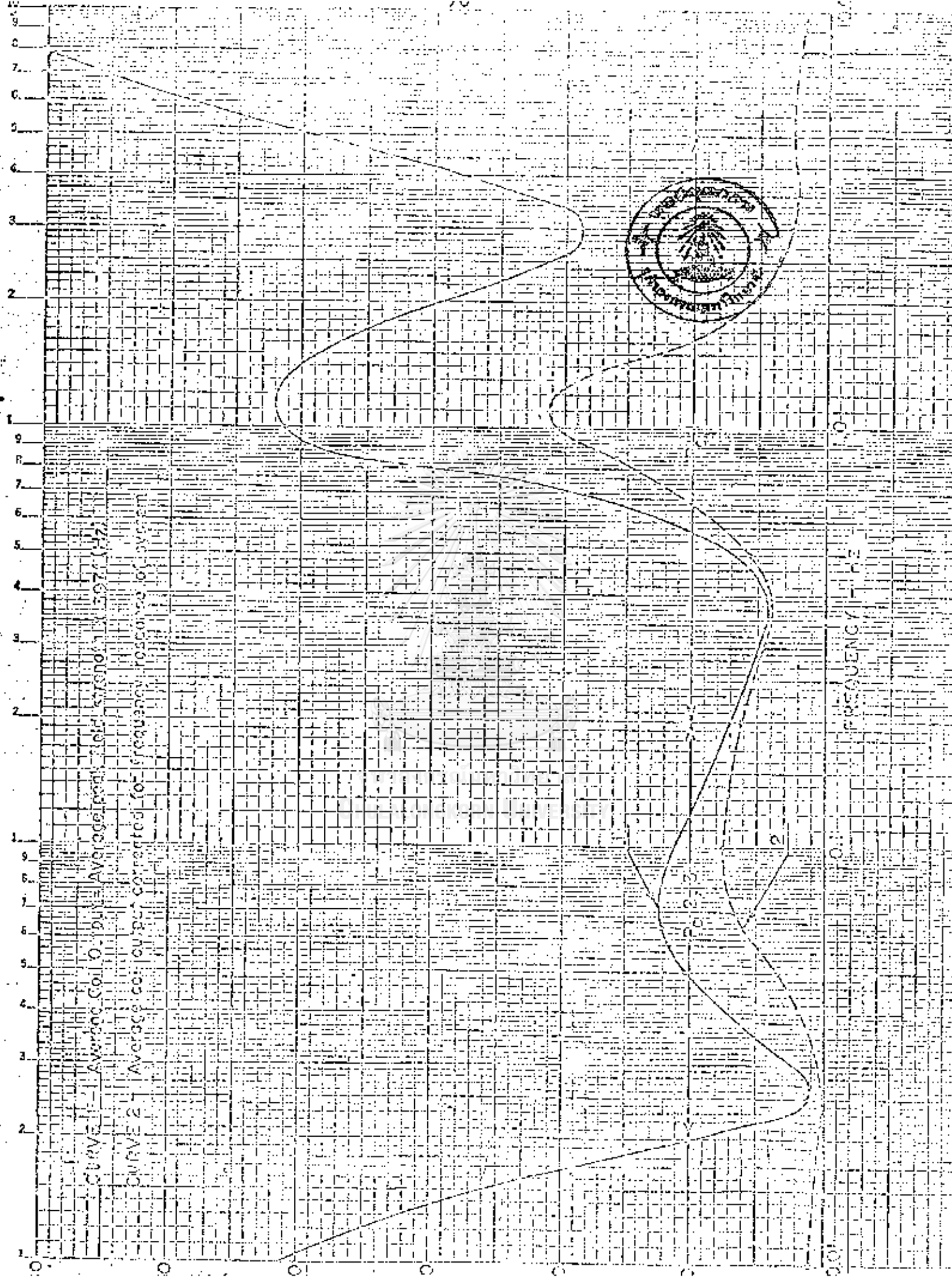


FIG. 157. FREQUENCY RESPONSE OF 60 HZ NOTCH FILTER AND ATTENUATOR

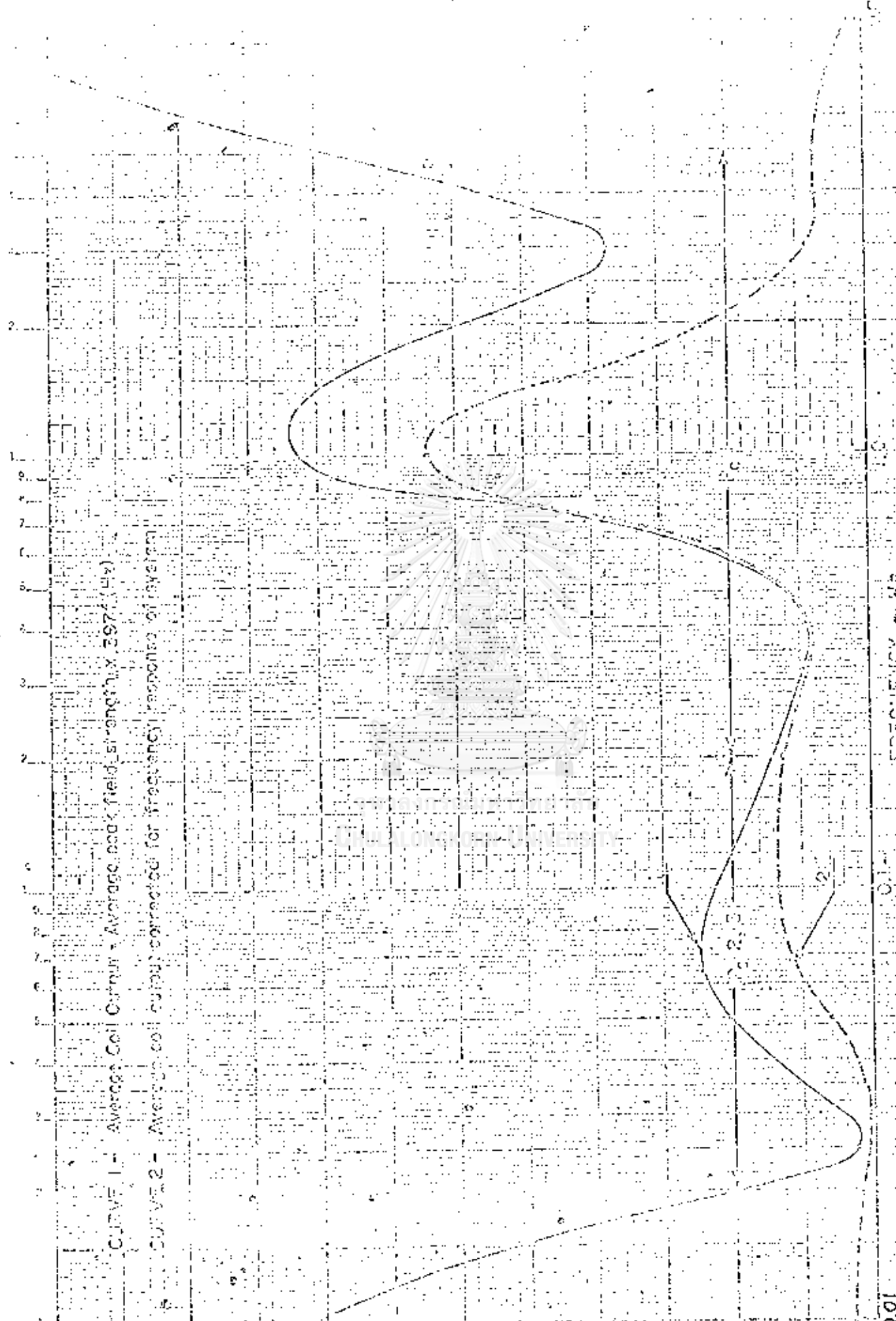


CURVE 1 - Average coil output (averaged) field crystal 1507 (H2)

CURVE 2 - Average coil output corrected for frequency response of system

FREQUENCY - Hz





CURVE 1 - Average Coil Output - Average peak field strength X 397.7 (Hz)

CURVE 2 - Average coil output corrected for frequency response of system

FREQUENCY - Hz

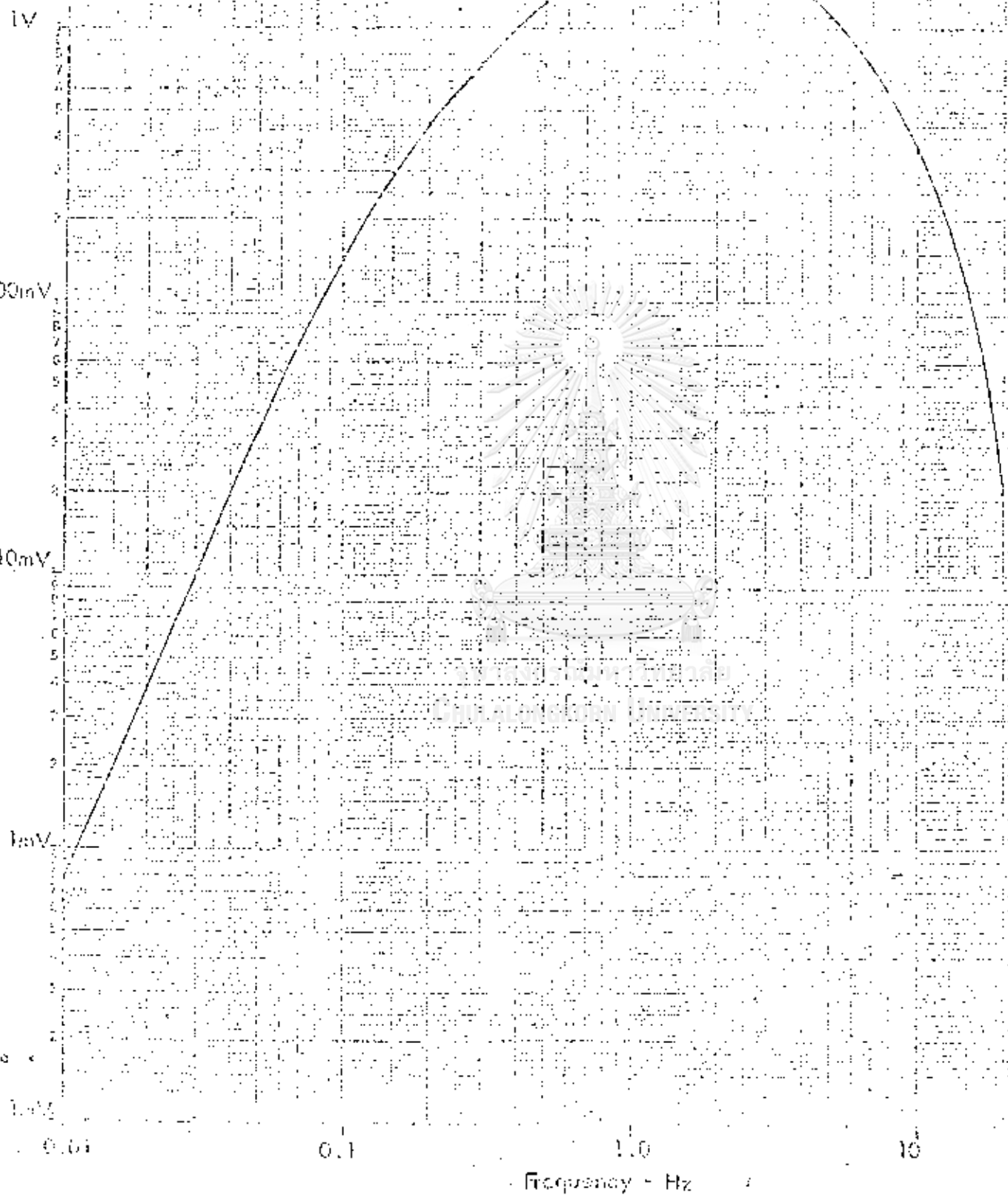


FIG. 17a. MAGNETIC RESPONSE OF MAGNETIC RECORDING SYSTEM
 Output Level Produced By 1V Oscillation - Total Amplification of 10⁶

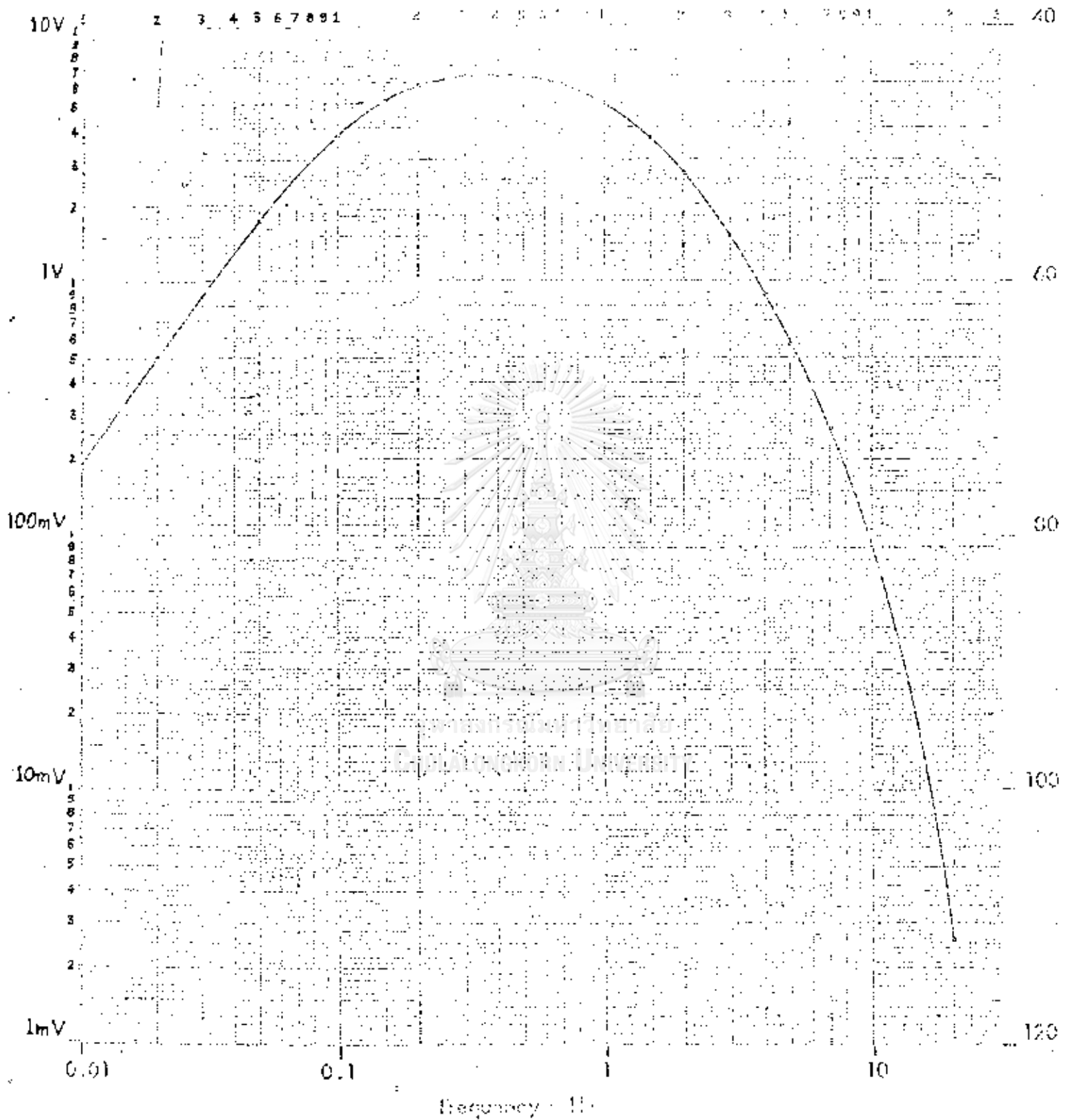


FIG. 116. FREQUENCY RESPONSE OF MAGNETIC RECORDING SYSTEM
Output for Input Oscillation of 3mV and Total Amplification of 10^5

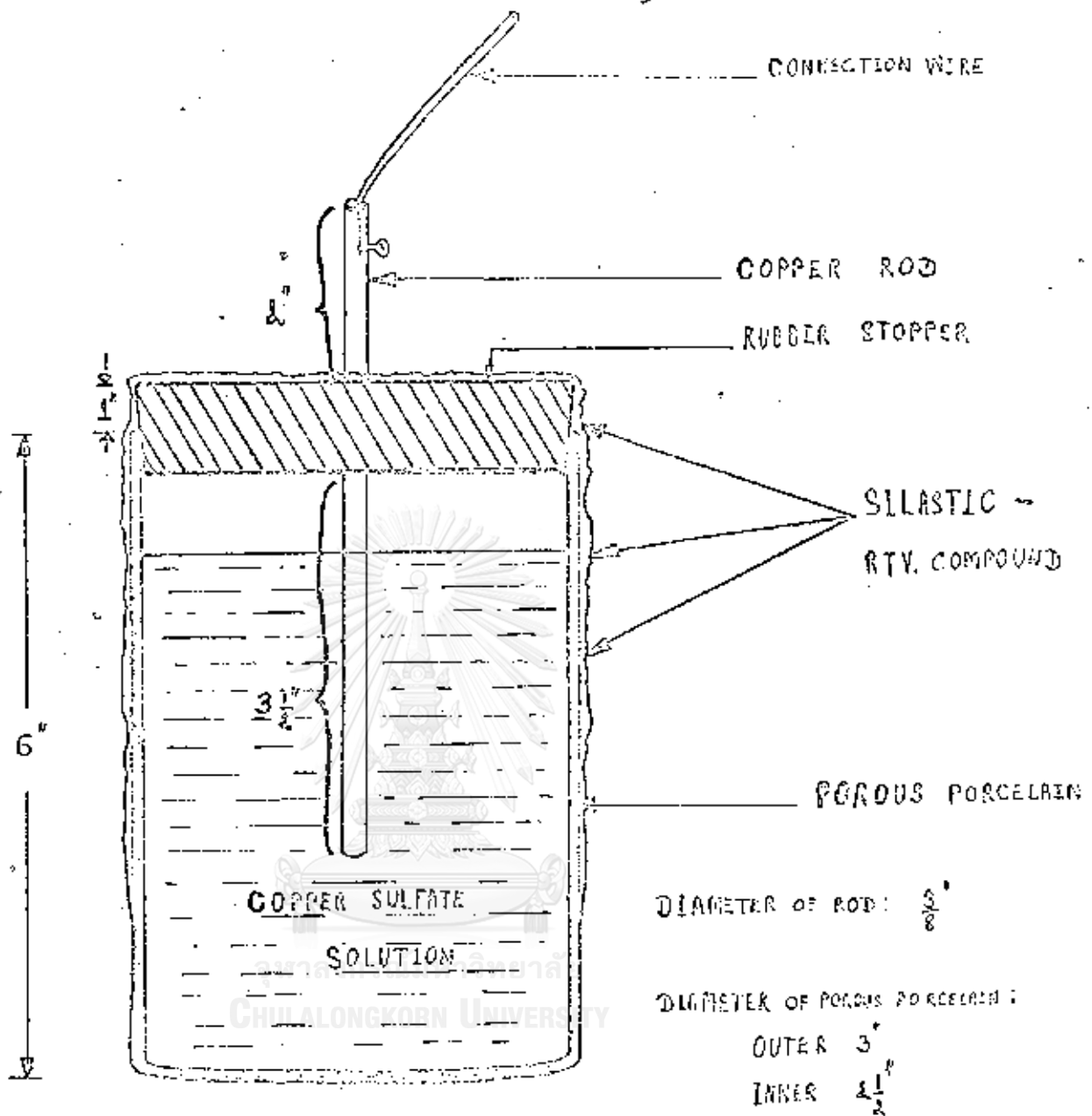


FIG. 18 C. NON-POLARIZING ELECTRODE. (COPPER ELECTRODE)

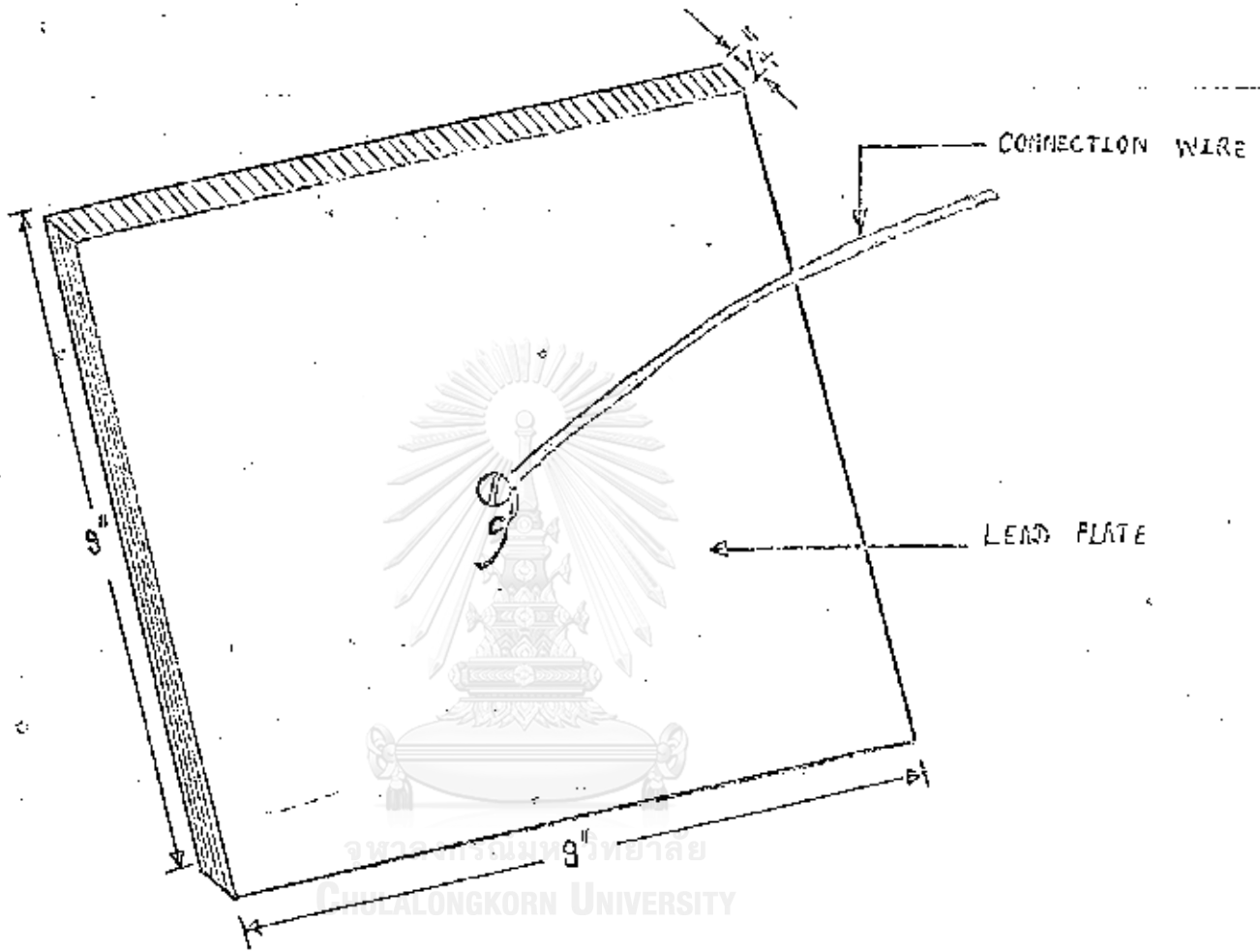


FIG. 18 b. "LEAD PLATES" ELECTRODE.

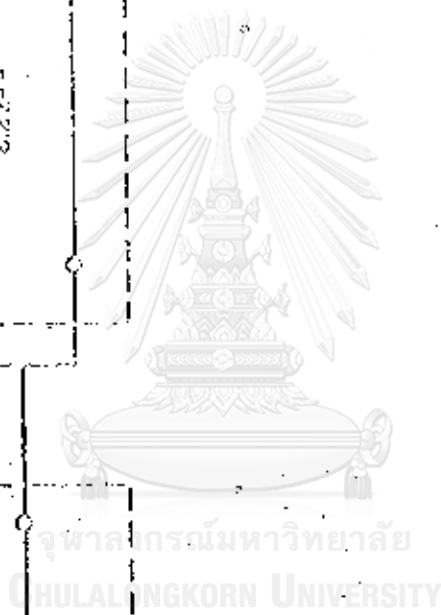
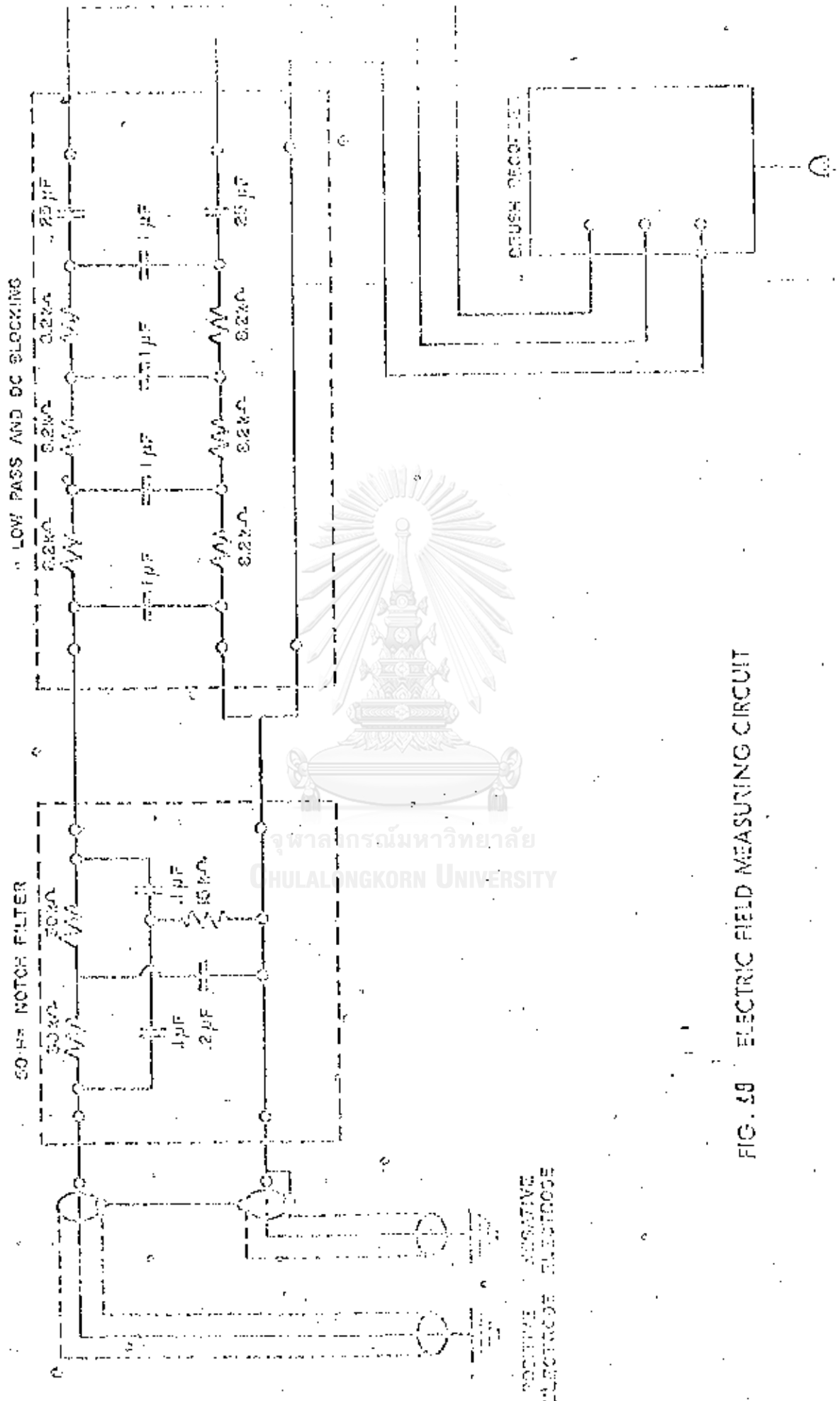


FIG. 59 ELECTRIC FIELD MEASURING CIRCUIT

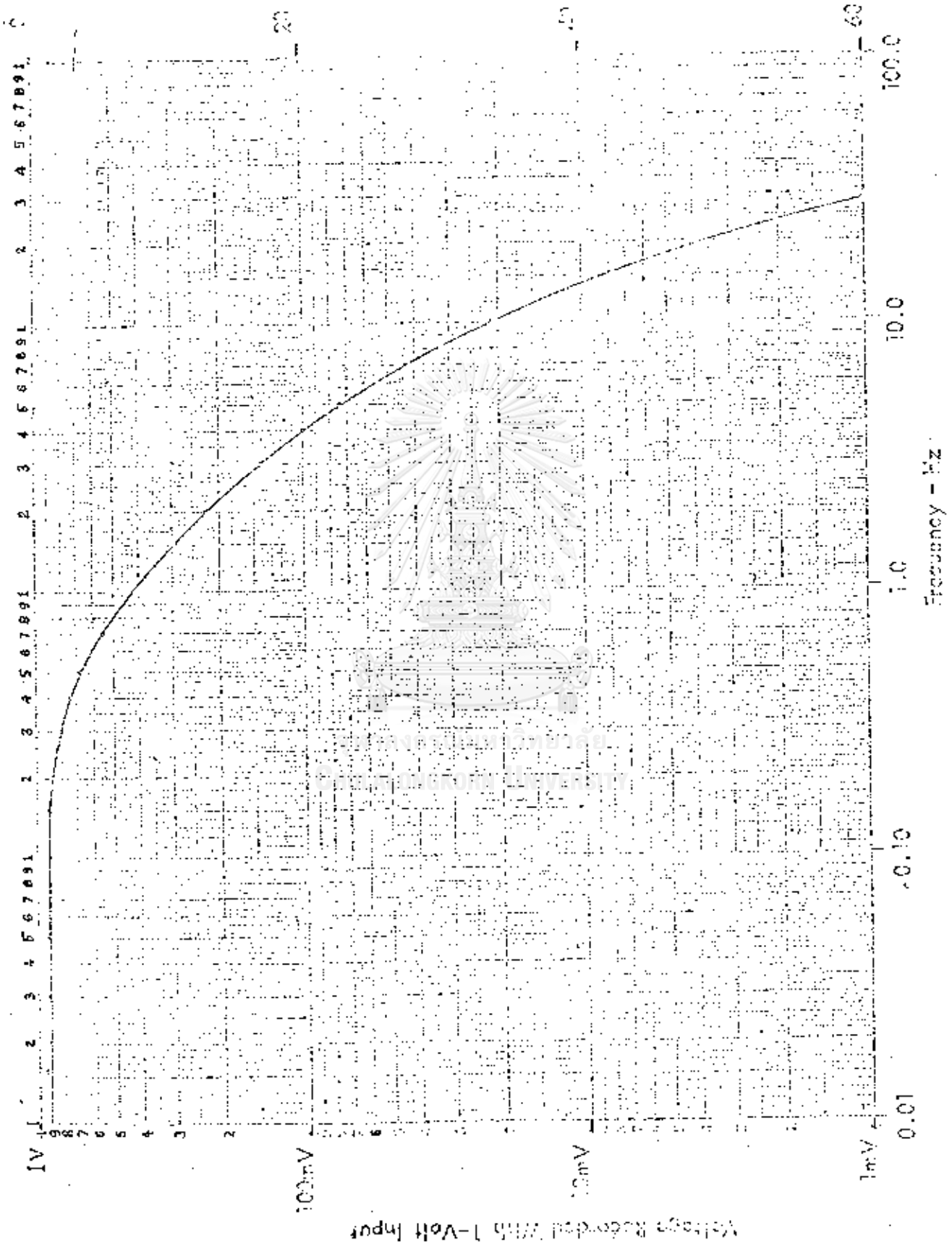
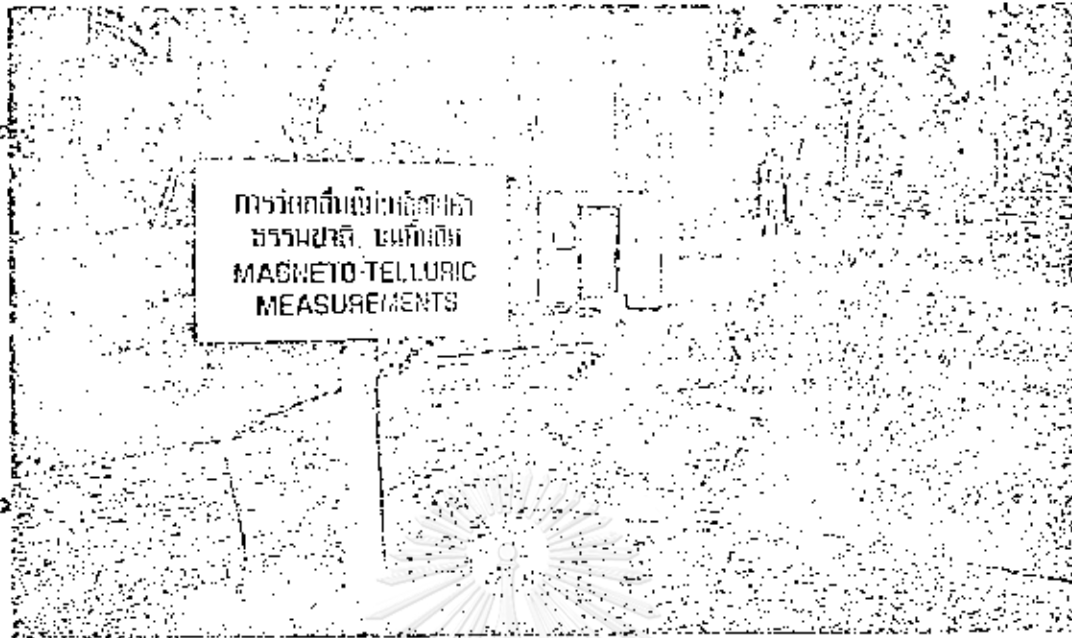


FIG. 3.0 OVERALL RESPONSE OF ELECTRIC FIELD MEASURING SYSTEM



Van and Surroundings



Interior with Instrumentation

FIG. 21 INSTRUMENT VAN AT TREND SITE

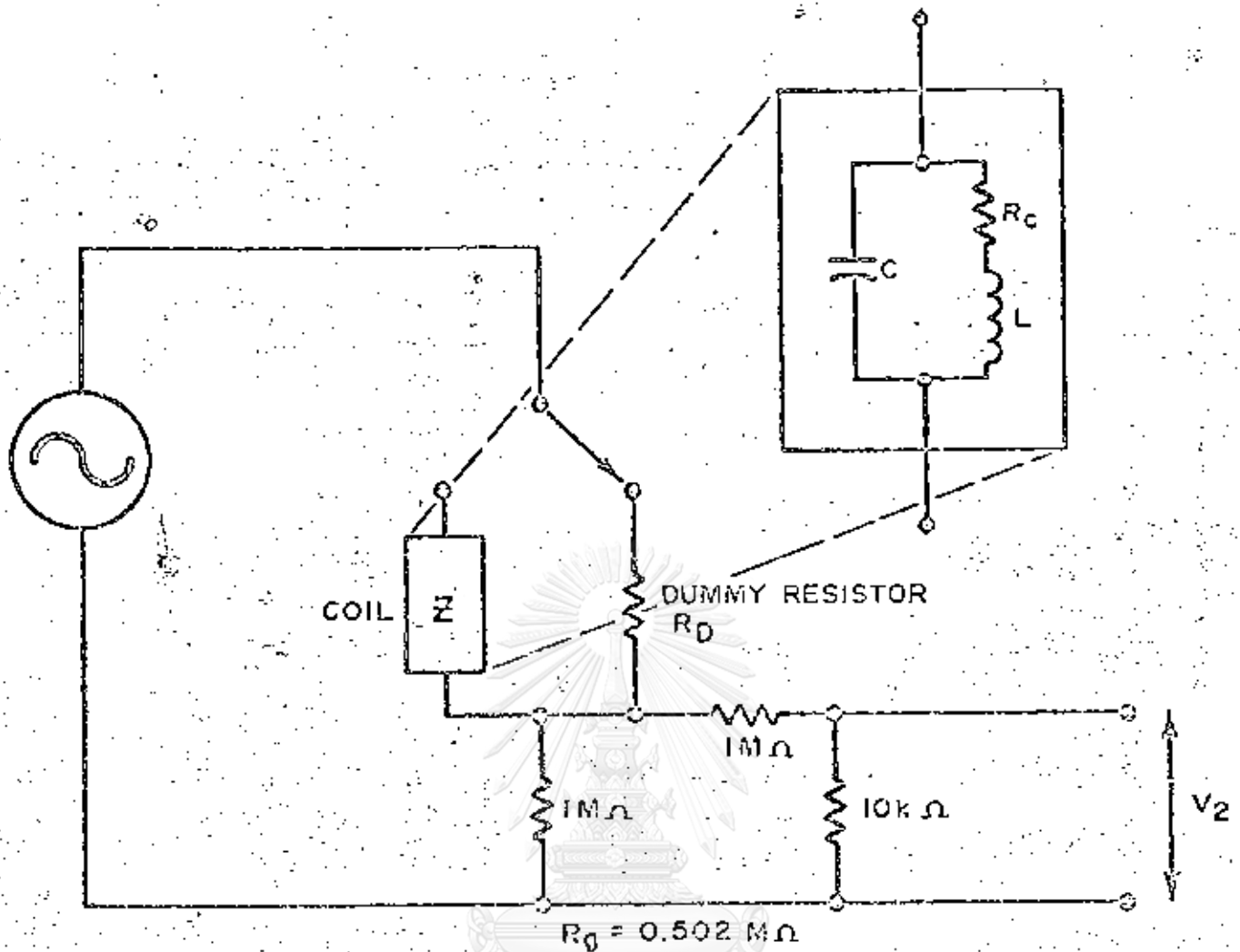


FIG. 22. COIL CALIBRATION CIRCUIT AFTER CAMPBELL (1959)



VITA

Name Ampai Phongsatha
Birthplace Patharam, Rejburi
Degrees B.Sc. (Hons.) in Physics, April, 1968
Chulalongkorn University
Bangkok, Thailand
Graduate Scholarship Applied Scientific Research
Cooperation of Thailand
Bangkok, Thailand
1968-1970.



จุฬาลงกรณ์มหาวิทยาลัย
CHULALONGKORN UNIVERSITY